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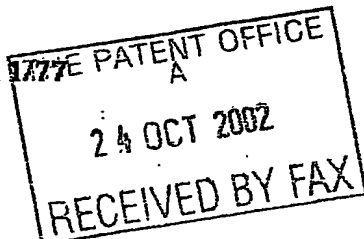
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1. Your reference

02.075-ipw/ph

2. Patent application number

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0224757.5

3. Full name, address and postcode of the or of each applicant (underline all surnames)

IPWireless, Inc.
1001 Bayhill Drive, 2nd Floor
San Bruno, California
CA 94066

Patents ADP number (If you know it)

If the applicant is a corporate body, give the country/state of its incorporation

USA, Delaware

8169401002

4. Title of the invention

METHOD AND ARRANGEMENT FOR CHANNEL
ESTIMATION IN A WIRELESS COMMUNICATION
SYSTEM

5. Name of your agent (If you have one)

Peter Hudson

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Patents ADP number (If you know it)

7987423001

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Country

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7. If this application is divided or otherwise derived from an earlier UK application, give the number and the filing date of the earlier application

Number of earlier application

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- a) any applicant named in part 3 is not an inventor, or
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Description	15
Claim(s)	5
Abstract	1
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Priority documents

Translations of priority documents

Statement of inventorship and right to grant of a patent (Patents Form 7/77) 3

Request for preliminary examination and search (Patents Form 9/77) 1

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Any other documents (please specify)

11. I/We request the grant of a patent on the basis of this application.

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Date

Peter L. Hudson

24 October 2002

12. Name and daytime telephone number of person to contact in the United Kingdom

Peter Hudson

01420 562565

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DUPLICATE

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METHOD AND ARRANGEMENT FOR CHANNEL ESTIMATION IN A
WIRELESS COMMUNICATION SYSTEM

5 **Field of the Invention**

This invention relates to wireless communication systems,
and particularly (though not exclusively) to UMTS
(Universal Mobile Telecommunication System) Terrestrial
10 Radio Access (UTRA) systems operating in Time Division
Duplex (TDD) mode.

Background of the Invention

15

In UTRA TDD, new User Equipment (UE) firstly synchronises
with the network and then transmits a random access burst
using the Physical Random Access Channel (PRACH). The
PRACH burst is actually received at the Node B (UMTS base
20 station) a time t (directly proportional to the distance
between the UE and Node B) later. A guard period is thus
required in order to avoid interference at the Node B
between the PRACH burst and another burst in the
subsequent timeslot. The size of the guard period
25 effectively limits the cell radius under normal
operation.

However, the network receiver (Node B) attempts to detect
the random access burst by identifying which of a
30 possible finite set of training sequences (midambles) was
transmitted by the UE, and typically this operation is

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performed by correlating the appropriate received samples with a local replica of each of the allowable training sequences. From each of the correlator outputs the presence of PRACH burst(s) with that particular training
5 sequence can be ascertained. Due to the construction of the training sequences from a single periodic base code, a high probability of false PRACH detection is experienced if the cell radius (allowable distance between UE and Node B) is allowed to be too large.

10

The maximum cell size is thus significantly limited below that allowed by the duration of the guard period, and is consequently not ideally suited to coverage of wide areas.

15

Although within UTRAN there currently exists an option to only use the odd-numbered midambles derived from a single periodic code, the resultant cell size is still not ideally suited to wide area coverage and does not take
20 full advantage of the PRACH burst guard period duration.

An alternative to the above approach for channel estimation could be to employ a zero-forcing channel estimate. However, in an asynchronous CDMA system with a
25 potentially large cell radius, a zero-forcing channel estimate would result in a degradation in signal-to-noise ratio too high for the reliable detection and demodulation of the PRACH bursts.

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A need therefore exists for PRACH detection in a wireless communication system wherein the abovementioned disadvantage(s) may be alleviated.

5

Statement of Invention

In accordance with a first aspect of the present invention there is provided an arrangement, for channel
10 estimation in a wireless communication system, as claimed in claim 1.

In accordance with a second aspect of the present invention there is provided a method, for channel
15 estimation in a wireless communication system, as claimed in claim 8.

In accordance with a third aspect of the present invention there is provided a method, for channel
20 estimation in a wireless communication system, as claimed in claim 19.

Brief Description of the Drawings

25

One method and arrangement for PRACH detection in a UTRA TDD system incorporating the present invention will now be described, by way of example only, with reference to the accompanying drawings, in which:

30

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FIG. 1 shows a block schematic representation of PRACH burst structure within UTRA TDD mode at 3.84 Mcps;

5 FIG. 2 shows a block schematic representation illustrating training sequence construction from base code;

FIGS. 3A-3D show waveform diagrams illustrating
10 respective correlator outputs for training sequences $m^{(1)}$ to $m^{(4)}$ with training sequence $m^{(1)}$ present;

FIG. 4 shows a block schematic diagram of an arrangement for asynchronous CDMA channel estimation
15 incorporating the present invention; and

FIG. 5 shows a flow-chart diagram illustrating a method used in the system of FIG. 4.

20

Description of Preferred Embodiment

In UTRA TDD (as specified in 3GPP Technical Specification TS25.221, 'Physical channels and mapping of transport
25 channels onto physical channels (TDD)', Version 3.10.0), new User Equipment (UE) firstly synchronises with the network and then transmits a random access burst using the Physical Random Access Channel (PRACH). The network receiver (Node B) attempts to detect the random access
30 burst by identifying which of a possible finite set of training sequences (midambles) was transmitted by the UE.

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Due to the construction of the training sequences from a single periodic base code, a high probability of false PRACH detection is experienced if the cell radius is allowed to be too large. FIG. 1 illustrates the format of the PRACH burst 100 in UTRA TDD mode at a chip rate of 3.84 Mcps. The PRACH burst 100 has a total length of 2560 chips, comprising:

- a first data symbol portion 110, of length 976 chips;
- a midamble portion 120 (which will be discussed in greater detail below), of length 512 chips;
- a second data symbol portion 130, of length 880 chips; and
- a guard period portion 140, of length 192 chips, where no signal is transmitted.

The UE initially has no knowledge of its distance from the Node B, and transmits its PRACH burst at the beginning of the appropriate timeslot. The PRACH burst is actually received at the Node B a time t later, related to the distance between the UE and Node B, t being given by the equation:

$$t = \frac{2 \times \text{distance}}{\text{speed of light}}$$

- The guard period 140 is thus required in order to avoid interference at the Node B between the PRACH burst and another burst in the subsequent timeslot. The size of the guard period effectively limits the cell radius under normal operation. For a typical chip rate of 3.84 Mcps

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this cell radius can be determined by re-arranging the above equation, to reveal a distance of 7.5Km.

The midamble portion 120 of the PRACH burst is chosen at random from a finite set of available training sequences. The available training sequences are known *a priori* at the Node B, and consequently the Node B can test each of the sequences to establish if a PRACH burst with that training sequence is present.

Each of the training sequences to be used within a cell for PRACH bursts is related to one of two base sequences of length P chips. The sequences related to one of these particular base sequences, mp 210, are obtained by periodically extending the base sequence and then selecting L_m chips every W chips. This process is repeated up to K times, as shown in FIG. 2, thus obtaining up to K midambles 220 from a single base code.

As an example of the values of the parameters in the outlined method of training sequence construction, UTRA TDD mode of operation at 3.84 Mcps may be considered:

The period of the base sequence, $P=456$ chips.

The length of the training sequences, $L_m=512$ chips.

Number of training sequences from a single base sequence, $K=8$.

The shift in base sequence between training sequences, $W=57$.

As can be seen from the above, the midamble length is $P+W-1$ as opposed to P chips. This is due to the fact

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that the midamble is inserted into the burst between 2 data payloads (portions 110 and 130 in FIG. 1), and thus the beginning of the midamble can suffer from intersymbol interference from the first data payload. For this reason, channel estimation is typically performed on the last P chips of the midamble.

The Node B has to decide which, if any, of the allowable training sequences have been transmitted in the timeslot(s) in which PRACH bursts are located. Typically, this operation is performed by correlating the appropriate received samples with a local replica of each of the allowable training sequences. From each of the correlator outputs the presence of PRACH burst(s) with that particular training sequence can be ascertained.

This process is demonstrated in FIG. 3A for UTRA TDD mode of operation at 3.84 Mcps. A PRACH burst with midamble $m^{(1)}$ is transmitted and correlated with the last P chips of a local replica to provide a channel estimation peak of magnitude P at correlator output position P . However, from FIG. 3B, it can also be noted that the output of the correlation with the local replica of midamble $m^{(2)}$ has two peaks at locations of +57 and -399 chips from the peak position in the correlation output with midamble $m^{(1)}$, i.e., P . These peaks, the cross-correlation terms between midambles $m^{(1)}$ and $m^{(2)}$, are the result of the construction of the midambles from a single periodic base code.

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This process is further demonstrated in FIG. 3C and FIG. 3D, where the cross-correlation peaks due to the correlation of midamble $m^{(1)}$ with midambles $m^{(3)}$ and $m^{(4)}$ respectively are displayed. As noted, in FIG. 3 only midamble $m^{(1)}$ is actually present; thus, the additional peaks in the other correlator outputs represent falsely detected PRACH bursts or a potential source of interference to any additional PRACH transmission channel estimates with different midambles.

10

As a consequence of the above discussion, it can be understood that in order to avoid the undesirable effects of the cross-correlation peaks, the maximum distance that a UE should be from a Node B should not exceed the W chip difference between the desired correlation peak and the first cross-correlation peak. However 57 chips at 3.84Mcps corresponds to:

$$\frac{57}{3.84 \times 10^6} \cdot \frac{\text{speed of light}}{2} = 2.225 \text{ Km}$$

20 The maximum cell size is thus limited to this radius, which is drastically reduced from the 7.5Km allowed by the duration of the guard period, and is consequently not ideally suited to coverage of wide areas.

25 It may be noted that within UTRAN there currently exists an option to only use the odd-numbered midambles derived from a single periodic code. Comparing FIG. 3A and FIG. 3C, it can be seen that this would increase the maximum distance between a UE and a Node B to 4.45 km (114 chips). However, this cell size is still not

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ideally suited to wide area coverage and does not take full advantage of the PRACH burst guard period duration.

An alternative to the above approach for channel estimation could be to employ a zero-forcing channel estimate. Such an approach for a synchronous CDMA system is described in the publication by Bernd Steiner and Peter Jung, 'Uplink channel estimation in synchronous CDMA mobile radio systems with joint detection', PIMRC 1993, pp123-127. With regards to an asynchronous CDMA system, such as UTRA TDD presently under consideration, the approach described in this publication can be extended by a person of ordinary skill in the art without invention. Without going into mathematical details, with a zero-forcing approach knowledge of all possible midambles is incorporated into the channel estimation process for each of the midambles. For instance, with a correlation channel estimation, the correlator output for midamble $m^{(1)}$ requires knowledge of (local replica) midamble $m^{(1)}$. For a zero-forcing channel estimation the filter output for midamble $m^{(1)}$ requires knowledge of all possible midambles present, i.e., $m^{(1)}$ to $m^{(8)}$.

However, the well-known drawback of using a zero-forcing technique is its tendency to degrade the signal-to-noise ratio of the output channel estimation relative to that of a correlation channel estimate. This degradation grows exponentially with increasing channel estimation size, and for large cell radii can be several decibels. This problem is further exacerbated by the asynchronous nature of the CDMA system presently under consideration.

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In the asynchronous system it is not known *a priori* which part of the received samples contains the midamble, and thus a larger set of received samples must be chosen in order to ensure that the midamble has been captured.

5 However, this means that part of the PRACH burst data payload may have been included in the received samples, and this can be considered additional noise at the input to the channel estimator. Consequently, at the output of the channel estimator a further degradation of the
10 signal-to-noise ratio, due to the additional input noise, can be expected relative to that of the correlation channel estimate.

From the above discussion it is clear that in an
15 asynchronous CDMA system (such as UTRA TDD) with a potentially large cell radius, a zero-forcing channel estimate would result in too high a degradation in signal-to-noise ratio for the reliable detection and demodulation of the PRACH bursts.

20 Referring now to FIG. 4, a superior approach to asynchronous channel estimation within large cell radii is shown. In the channel estimator arrangement 400 in a Node B 410, a correlation channel estimator 420 forms
25 correlator channel estimates from received samples as described above. The output from the correlation channel estimator 420 is applied to a correlation peak identifier 430. The output of the correlation peak identifier 430 and the output of the correlation channel estimator 420
30 are applied to a cross-correlation peak remover 440. The cross-correlation peak remover 440 removes cross-

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correlation peaks from the output of the correlation channel estimator 420, without increasing the noise variance of the channel estimate, to produce an improved channel estimate output.

5

Based upon knowledge of the midamble construction from a single periodic base sequence, e.g., FIG. 2, an algorithm for post-processing (i.e., processing after the correlation channel estimator 420 forms correlator channel estimates from received samples as described above) is designed that is essentially able to clean up the channel estimates at the output of the correlators. The training sequences are extracted from a single periodic base code of period P chips at intervals of W chips. The length of the extracted midambles is L_m chips.

If a wanted correlation peak is present in the k^{th} correlator output (i.e., midamble $\underline{m}^{(k)}$) at position p , then each of the other correlator outputs will have a pair of cross-correlation peaks located at positions:

$$p+W \bmod(k-k',K) \text{ and } p+W \bmod(k-k',K)-P \quad (1)$$

where $k=1,\dots,K$

It is apparent that once a desired correlation peak has been identified from among the correlator outputs, the associated cross-correlation peaks may be cancelled from the other correlator outputs using the cross-correlation peak positions from (1) above. Furthermore, each of the cross-correlation peaks has a smaller magnitude than the desired correlation peak, thus making it possible to

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identify which peak in the correlator outputs is the desired one.

Referring now also to FIG. 5, a suitable, but not unique, method 500 of implementing the above algorithm is described below in terms of steps:

Step 1: form the correlation channel estimates
(510) for each of the allowable midambles $\underline{m}^{(n)}$ to $\underline{m}^{(N)}$.

Step 2: identify the largest magnitude peak
(520) across all the correlator outputs. For instance, assume this is located in correlator output k' at position p .

Step 3: cancel the cross-correlation peaks in
(530) all the other correlator outputs, i.e., $k \neq k'$ at locations given at (1).

Step 4: identify the next largest magnitude
(540) remaining peak across all updated correlator outputs that has not been previously identified. Go to Step 3.

It can be seen that the above algorithm iterates between Step 3 (530) and Step 4 (540). One could either iterate these steps a fixed or programmable number of times. One potential method would be to iterate the steps until the magnitude of the identified peak is below a programmable threshold.

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The post-processing of the correlator outputs can be performed in a number of potential ways, all of which exploit the knowledge of the construction of the midamble training sequences from a single periodic base code.

5

Additionally it should be noted that the described method of channel estimation with post-processing to remove unwanted cross-correlation peaks is suitable for other chip rates, and other midamble constructions. For instance, the period of the midamble base code is not restricted to 456 chips, the length of midamble is not restricted to 512 chips and the offsets for each midamble do not have to be multiples of 57 chips.

10

It will be appreciated that the method of channel estimation described above may be carried out in software running on a processor (not shown) in a Node B, and that the software may be provided as a computer program element carried on any suitable data carrier (also not shown) such as a magnetic or optical computer disc.

15

It will be also be appreciated that the method of channel estimation described above may alternatively be carried out in hardware, for example in the form of an integrated circuit (not shown) such as an FPGA (Field Programmable Gate Array) or ASIC (Application Specific Integrated Circuit) in a Node B.

20

Although the above method of channel estimation has been described in terms of chip spaced operation, it will be understood that the method may be employed in an over-

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sampled system. For instance, if the correlator outputs are provided at os samples per chip and the desired peak is identified at position p in the k^{th} correlator output, the other correlator outputs will have a pair of cross-correlation peaks located at positions:

$$p + os \cdot W \bmod(k - K, K) \text{ and } p + os \cdot (W \bmod(k - k', K) - P)$$

where $k = 1, \dots, K$

Implementation of the cross-correlation peak post-processing as outlined removes the unwanted peaks from the correlator outputs. This also removes the restriction upon cell size due to the unwanted cross-correlation peaks, and thus the maximum cell size is governed by the duration of the guard period. If a cell size in excess of 7.5 km is required then it would be possible for UTRAN to ensure that no transmissions were scheduled for the timeslot following the allocated PRACH timeslot. In this manner, the guard period on the PRACH burst would be effectively extended to $192 + 2560$ chips which corresponds to a cell size in excess of 100km.

It will be understood that the method and arrangement for channel estimation in a wireless communication system described above provides the following advantages:

- Low probability of false detection.
- No degradation in the signal-to-noise ratio of the channel estimates.

It should be noted that although the invention is described in relation to the current UTRA TDD mode of

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operation at 3.84 Mcps, it can easily be applied to other scenarios where a burst structure with midambles or preambles formed from a single periodic code are employed. In particular, the described method of PRACH
5 detection would be applicable to UTRA TDD modes with differing chip rates, both current and proposed.

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Claims

1. An arrangement for channel estimation in a wireless communication system, the arrangement comprising:
- 5 correlation channel estimation means for receiving input signals representative of channel information and for producing therefrom correlation channel estimate signals;
- correlation peak identification means coupled
- 10 to the correlation channel estimation means for deriving from the correlation channel estimate signals representative of correlation peaks; and
- cross-correlation peak removal means coupled to the correlation channel estimation means and to the
- 15 correlation peak identification means for removing cross-correlation peaks from the correlation channel estimate signals to produce improved channel estimate signals.
- 20 2. The arrangement of claim 1 wherein the correlation peak identification means comprises cross-correlation peak identification means for identifying a cross-correlation peak as having a smaller magnitude than a correlation peak.
- 25 3. The arrangement of claim 1 or 2 wherein the input signals representative of channel information comprise signal portions constructed from a single periodic base code.
- 30

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4. The arrangement of claim 3 wherein the signal portions comprise midambles.

5. The arrangement of any preceding claim wherein the wireless communication system is a UMTS system.

6. The arrangement of claim 5 wherein the UMTS system is a UTRA TDD system.

7. The arrangement of claim 6 wherein the input signals comprise random access PRACH bursts.

8. A method for channel estimation in a wireless communication system, the method comprising:

15 providing correlation channel estimation means receiving input signals representative of channel information and producing therefrom correlation channel estimate signals;

20 providing correlation peak identification means coupled to the correlation channel estimation means, the correlation peak identification means deriving from the correlation channel estimate signals representative of correlation peaks; and

25 providing cross-correlation peak removal means coupled to the correlation channel estimation means and to the correlation peak identification means, the cross-correlation peak removal means removing cross-correlation peaks from the correlation channel estimate signals to produce improved channel
30 estimate signals.

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9. The method of claim 8 wherein the correlation peak identification means comprises cross-correlation peak identification means identifying a cross-correlation peak as having a smaller magnitude than a correlation peak.
- 5
10. The method of claim 8 or 9 wherein the input signals representative of channel information comprise signal portions constructed from a single periodic base code.
- 10
11. The method of claim 10 wherein the signal portions comprise midambles.
12. The method of any one of claims 8-11 wherein the
- 15 wireless communication system is a UMTS system.
13. The method of claim 12 wherein the UMTS system is a UTRA TDD system.
14. The method of claim 13 wherein the input signals
- 20 comprise random access PRACH bursts.
15. The method of any one of claims 8-14 wherein the step of providing cross-correlation peak removal means
- 25 comprises repeatedly cancelling cross-correlation peaks at locations other than that of an identified peak and identifying the next largest magnitude remaining peak.
16. The method of claim 15 wherein the step of
- 30 repeatedly cancelling and identifying is performed a predetermined number of times.

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17. The method of claim 15 wherein the step of repeatedly cancelling and identifying is performed until an identified peak has a magnitude less than a
5 predetermined value.
18. The method of any one of claims 8-17 further comprising ensuring that no transmission occurs in a timeslot immediately following that in which channel
10 estimation is performed.
19. A method for channel estimation in a wireless communication system, the method comprising:
providing correlation channel estimation means
15 receiving input signals representative of channel information and producing therefrom correlation channel estimate signals; and
ensuring that no transmission occurs in a timeslot immediately following that in which channel
20 estimation is performed.
20. A base station for use in a wireless communication system comprising an arrangement as claimed in any one of claims 1-7.
25
21. An integrated circuit comprising the arrangement of any one of claims 1-7.
22. A computer program element comprising computer
30 program means for performing the method of any one of claims 8-19.

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23. An arrangement, for channel estimation in a wireless communication system, substantially as hereinbefore described with reference to the accompanying drawings.

5

24. A method, for channel estimation in a wireless communication system, substantially as hereinbefore described with reference to the accompanying drawings.

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Abstract

METHOD AND ARRANGEMENT FOR CHANNEL ESTIMATION IN A
WIRELESS COMMUNICATION SYSTEM

5

A method and arrangement (100) for PRACH burst channel detection in a UTRA TDD wireless communication system in which training sequences are constructed from a single periodic base code. Unwanted cross-correlation peaks, having magnitude less than correlation peaks, are removed (440) from the correlator outputs, maintaining optimal signal-to-noise ratio of the channel estimates, providing a low probability of false detection, and extending the cell size of a CDMA network to that determined by the guard period duration. The cell size can be extended further by ensuring that no transmissions are scheduled for the timeslot subsequent to that in which the channel estimation bursts are scheduled.

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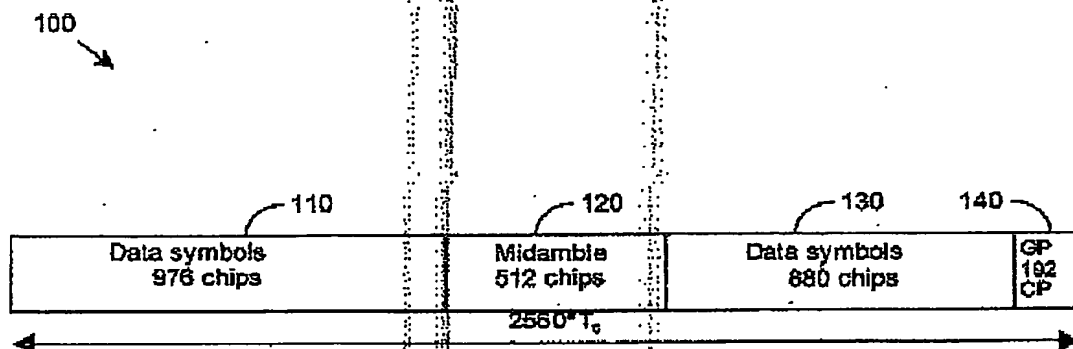


FIG. 1
Prior Art

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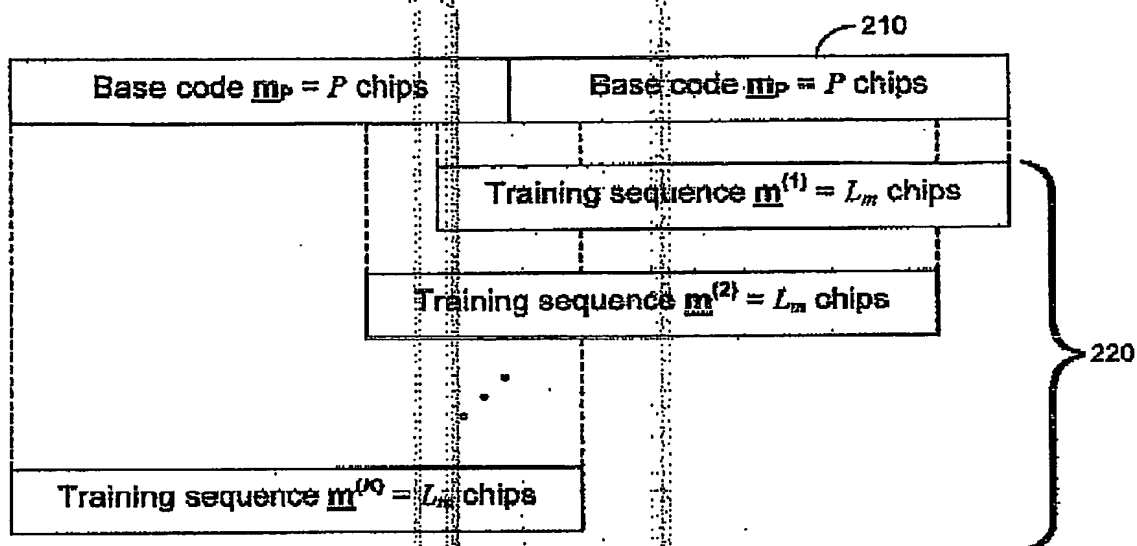
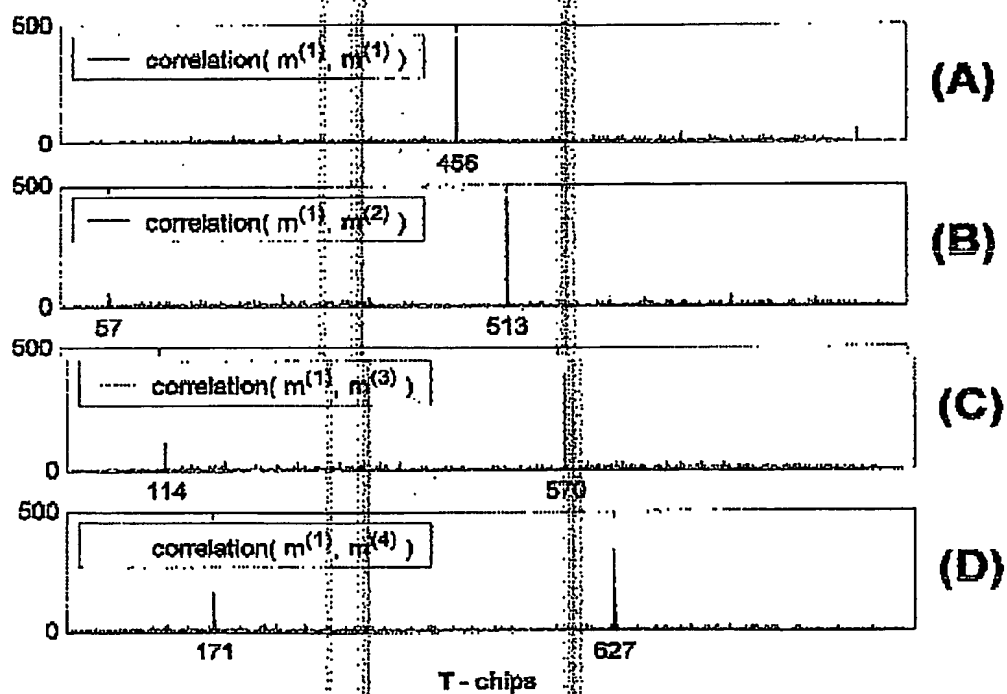


FIG. 2
Prior Art

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**FIG. 3**
Prior Art

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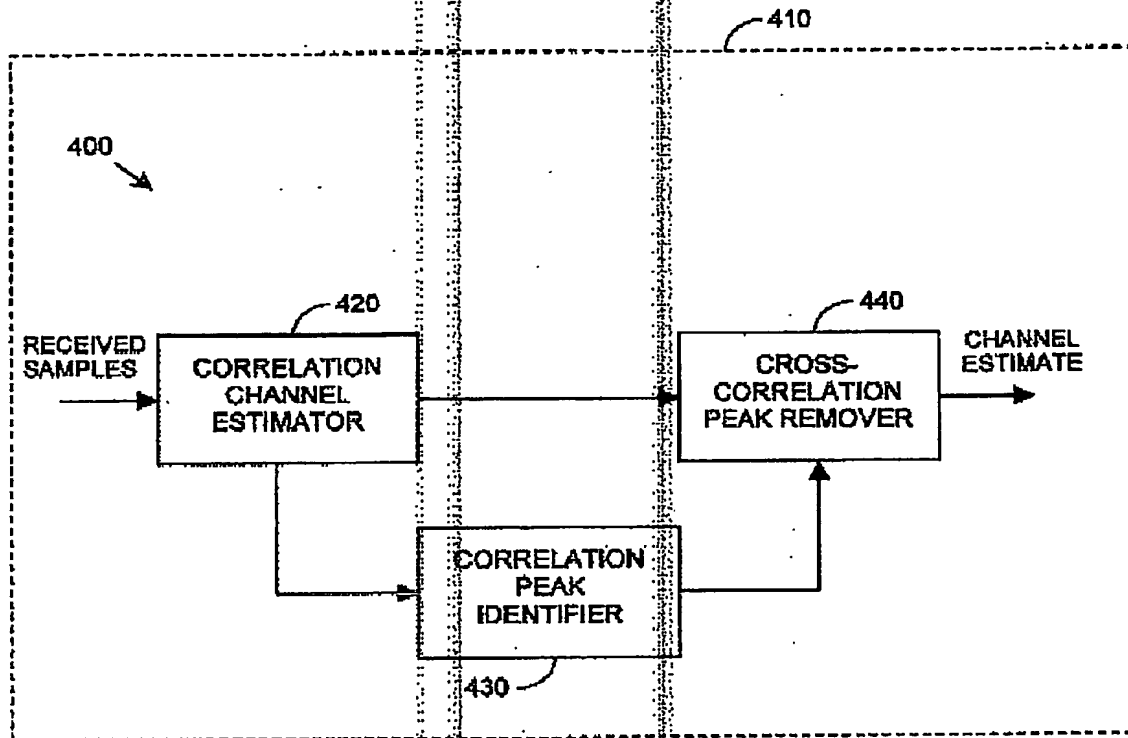


FIG. 4

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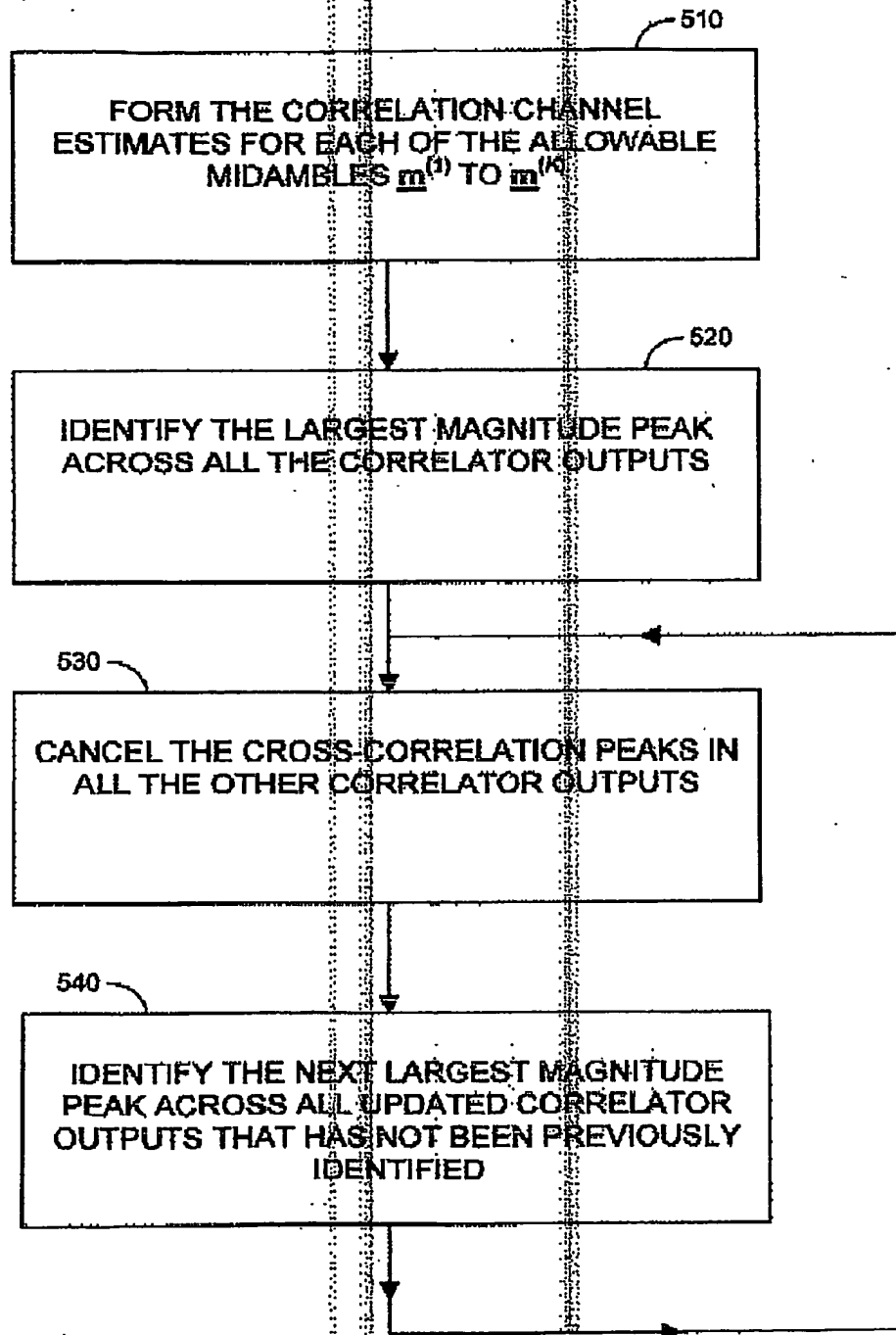
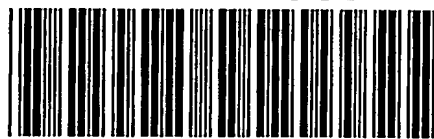


FIG. 5

PCI Application
GB0304587



GB0304587